**GENERAL DESCRIPTION**

The MLT04 is a complete, four-channel, voltage output analog multiplier packaged in an 18-pin DIP or SOIC-18. These complete multipliers are ideal for general purpose applications such as voltage controlled amplifiers, variable active filters, “zipper” noise free audio level adjustment, and automatic gain control. Other applications include cost-effective multiple-channel power calculations \(I \times V\), polynomial correction generation, and low frequency modulation. The MLT04 multiplier is ideally suited for generating complex, high-order waveforms especially suitable for geometry correction in high-resolution CRT display systems.

Fabricated in a complementary bipolar process, the MLT04 includes four 4-quadrant multiplying cells which have been laser-trimmed for accuracy. A precision internal bandgap reference normalizes signal computation to a 0.4 scale factor. Drift over temperature is under 0.005%/°C. Spot noise voltage of 0.3 µV/√Hz results in a THD + Noise performance of 0.02% (LPF = 22 kHz) for the lower distortion Y channel. The four 8 MHz channels consume a total of 150 mW of quiescent power.

The MLT04 is available in 18-pin plastic DIP, and SOIC-18 surface mount packages. All parts are offered in the extended industrial temperature range (–40°C to +85°C).

**APPLICATIONS**

- Geometry Correction in High-Resolution CRT Displays
- Waveform Modulation & Generation
- Voltage Controlled Amplifiers
- Automatic Gain Control
- Modulation and Demodulation

**FEATURES**

- Four Independent Channels
- Voltage IN, Voltage OUT
- No External Parts Required
- 8 MHz Bandwidth
- Four-Quadrant Multiplication
- Voltage Output; \(W = (X \times Y)/2.5\) V
- 0.2% Typical Linearity Error on X or Y Inputs
- Excellent Temperature Stability: 0.005%
- ±2.5 V Analog Input Range
- Operates from ±5 V Supplies
- Low Power Dissipation: 150 mW typ
- Spice Model Available

**REV. B**

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**ORDERING INFORMATION**

For die specifications contact your local Analog sales office. The MLT04 contains 211 transistors.

**ABSOLUTE MAXIMUM RATINGS**

Supply Voltages $V_{CC}$, $V_{EE}$ to GND
- $V_{CC}$: +7 V
- $V_{EE}$: -7 V

Inputs $x_i$, $y_i$
- $V_{CC}$, $V_{EE}$
- $V_{EE}$, $V_{CC}$

Outputs $W_i$
- $V_{CC}$, $V_{EE}$
- $V_{EE}$, $V_{CC}$

Operating Temperature Range
- -40°C to +85°C

Maximum Junction Temperature ($T_{J, max}$)
- +150°C

Storage Temperature
- -65°C to +150°C

Lead Temperature (Soldering, 10 sec)
- +300°C

Package Power Dissipation
- $P_{DISS} = \frac{5.25 \times V_{CC} + 5.25 \times V_{EE}}{2}$
- Calculated: $5.25 \times V_{CC} + 5.25 \times V_{EE} = 150 \text{ mW}$
- $150 \text{ mW}$

Supply Sensitivity
- $V_{CC} = 5.25 \text{ V}$
- $V_{EE} = -5.25 \text{ V}$
- +4.75 V
- $\pm 5.25 \text{ V}$

Supply Voltage Range
- $V_{CC}$
- $V_{EE}$

NOTES
1. *Specifications apply to all four multipliers.*
2. Error is measured as a percent of the ±2.5 V full scale, i.e., 1% FS = 25 mV.
3. Scale Factor $K$ is an internally set constant in the multiplier transfer equation $W = K \times X \times Y$.

Specifications subject to change without notice.

REV. B
FUNCTIONAL DESCRIPTION

The MLT04 is a low cost quad, 4-quadrant analog multiplier with single-ended voltage inputs and voltage outputs. The functional block diagram for each of the multipliers is illustrated in Figure 3. Due to packaging constraints, access to internal nodes for externally adjusting scale factor, output offset voltage, or additional summing signals is not provided.

Each of the MLT04’s analog multipliers is based on a Gilbert cell multiplier configuration, a 1.23 V bandgap reference, and a unity-connected output amplifier. Multiplier scale factor is determined through a differential pair/trimmable resistor network external to the core. An equivalent circuit for each of the multipliers is shown in Figure 4.

Details of each multiplier’s output-stage amplifier are shown in Figure 5. The output stages idles at 200 µA, and the resistors in series with the emitters of the output stage are 25 Ω. The output stage can drive load capacitances up to 500 pF without oscillation. For loads greater than 500 pF, the outputs of the MLT04 should be isolated from the load capacitance with a 100 Ω resistor.

ANALOG MULTIPLIER ERROR SOURCES

Multiplier errors consist primarily of input and output offsets, scale factor errors, and nonlinearity in the multiplying core. An expression for the output of a real analog multiplier is given by:

\[ V_o = (K + \Delta K)(V_x + X_{os})(V_y + Y_{os}) + Z_{os} + f(X, Y) \]

where:
- \( K \) = Multiplier Scale Factor
- \( \Delta K \) = Scale Factor Error
- \( V_x \) = X-Input Signal
- \( X_{os} \) = X-Input Offset Voltage
- \( V_y \) = Y-Input Signal
- \( Y_{os} \) = Y-Input Offset Voltage
- \( Z_{os} \) = Multiplier Output Offset Voltage
- \( f(X, Y) \) = Nonlinearity

Executing the algebra to simplify the above expression yields expressions for all the errors in an analog multiplier:

<table>
<thead>
<tr>
<th>Term</th>
<th>Description</th>
<th>Dependence on Input</th>
</tr>
</thead>
<tbody>
<tr>
<td>( KV_xV_y )</td>
<td>True Product</td>
<td>Goes to Zero As Either or Both Inputs Go to Zero</td>
</tr>
<tr>
<td>( \Delta KV_xV_y )</td>
<td>Scale-Factor Error</td>
<td>Goes to Zero at ( V_x, V_y = 0 )</td>
</tr>
<tr>
<td>( V_xY_{os} )</td>
<td>Linear “X” Feedthrough Due to Y-Input Offset</td>
<td>Proportional to ( V_x )</td>
</tr>
<tr>
<td>( V_yX_{os} )</td>
<td>Linear “Y” Feedthrough Due to X-Input Offset</td>
<td>Proportional to ( V_y )</td>
</tr>
<tr>
<td>( X_{os}Y_{os} )</td>
<td>Output Offset Due to X-, Y-Input Offsets</td>
<td>Independent of ( V_x, V_y )</td>
</tr>
<tr>
<td>( Z_{os} )</td>
<td>Output Offset</td>
<td>Independent of ( V_x, V_y )</td>
</tr>
<tr>
<td>( f(X, Y) )</td>
<td>Nonlinearity</td>
<td>Depends on Both ( V_x, V_y ); Contains Terms Dependent on ( V_x, V_y ), Their Powers and Cross Products</td>
</tr>
</tbody>
</table>

As shown in the table, the primary static errors in an analog multiplier are input offset voltages, output offset voltage, scale factor, and nonlinearity. Of the four sources of error, only two are externally trimmable in the MLT04: the \( X \)- and \( Y \)-input offset voltages. Output offset voltage in the MLT04 is factory-trimmed to ±50 mV, and the scale factor is internally adjusted to ±2.5% of full scale. Input offset voltage errors can be eliminated by using the optional trim circuit of Figure 6. This scheme then reduces the net error to output offset, scale-factor (gain) error, and an irreducible nonlinearity component in the multiplying core.

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Feedthrough
In the ideal case, the output of the multiplier should be zero if either input is zero. In reality, some portion of the nonzero input will “feedthrough” the multiplier and appear at the output. This is caused by the product of the nonzero input and the offset voltage of the “zero” input. Introducing an offset equal to and opposite of the “zero” input offset voltage will null the linear component of the feedthrough. Residual feedthrough at the output of the multiplier is then irreducible core nonlinearity.

Typical X- and Y-input feedthrough curves for the MLT04 are shown in Figures 7 and 8, respectively. These curves illustrate MLT04 feedthrough after “zero” input offset voltage trim. Residual X-input feedthrough measures 0.08% of full scale, whereas residual Y-input feedthrough is almost immeasurable.

Nonlinearity
Multiplier core nonlinearity is the irreducible component of error. It is the difference between actual performance and “best-straight-line” theoretical output, for all pairs of input values. It is expressed as a percentage of full scale with all other dc errors nulled. Typical X- and Y-input nonlinearities for the MLT04 are shown in Figures 9 through 12. Worst-case X-input nonlinearity measured less than 0.2%, and Y-input nonlinearity measured better than 0.06%. For modulator/demodulator or mixer applications it is, therefore, recommended that the carrier be connected to the X-input while the signal is applied to the Y-input.
MLT04 - Typical Performance Characteristics

Figure 19. Feedthrough vs. Frequency

Figure 20. Crosstalk vs. Frequency

Figure 21. Gain Flatness vs. Frequency

Figure 22. Y-Input Small-Signal Transient Response, $C_L = 30 \, \text{pF}$

Figure 23. Y-Input Small-Signal Transient Response, $C_L = 100 \, \text{pF}$

Figure 24. Y-Input Large-Signal Transient Response, $C_L = 30 \, \text{pF}$

Figure 25. Y-Input Large-Signal Transient Response, $C_L = 100 \, \text{pF}$
Figure 26. THD + Noise vs. Input Signal Level

Figure 27. Linearity Error vs. Temperature

Figure 28. X-Input Gain Bandwidth vs. Temperature

Figure 29. Y-Input Gain Bandwidth vs. Temperature

Figure 30. Maximum Output Swing vs. Frequency

Figure 31. Maximum Output Swing vs. Resistive Load
Figure 32. Offset Voltage Distribution

Figure 33. Offset Voltage vs. Temperature

Figure 34. Scale Factor Distribution

Figure 35. Scale Factor vs. Temperature

Figure 36. Output Offset Voltage (Z_{OS}) Distribution

Figure 37. Output Offset Voltage (Z_{OS}) vs. Temperature
Figure 38. Supply Current vs. Temperature

Figure 39. Power Supply Rejection vs. Frequency

Figure 40. Linearity Error (LE) Distribution Accelerated by Burn-in

Figure 41. Output Voltage Offset ($Z_{oc}$) Distribution Accelerated by Burn-in

Figure 42. Scale Factor (K) Distribution Accelerated by Burn-in
**MLT04**

**APPLICATIONS**
The MLT04 is well suited for such applications as modulation/demodulation, automatic gain control, power measurement, analog computation, voltage-controlled amplifiers, frequency doublers, and geometry correction in CRT displays.

**Multiplier Connections**
Figure 43 illustrates the basic connections for multiplication. Each of the four independent multipliers has single-ended voltage inputs (X, Y) and a low impedance voltage output (W). Also, each multiplier has its own dedicated ground connection (GND) which is connected to the circuit’s analog common. For best performance, circuit layout should be compact with short component leads and well-bypassed supply voltage feeds. In applications where fewer than four multipliers are used, all unused analog inputs must be returned to the analog common.

**Squaring and Frequency Doubling**
As shown in Figure 44, squaring of an input signal, $V_{in}$, is achieved by connecting the X- and Y-inputs in parallel to produce an output of $V_{in}^2/2.5V$. The input may have either polarity, but the output will be positive.

The equation shows a dc term at the output which will vary strongly with the amplitude of the input, $V_{in}$. The output dc offset can be eliminated by capacitively coupling the MLT04’s output with a high-pass filter. For optimal spectral performance, the filter’s cutoff frequency should be chosen to eliminate the input fundamental frequency.

A source of error in this configuration is the offset voltages of the X and Y inputs. The input offset voltages produce cross products with the input signal to distort the output waveform. To circumvent this problem, Figure 45 illustrates the use of inverting amplifiers configured with an OP285 to provide a means by which the X- and Y-input offsets can be trimmed.

**Feedback Divider Connections**
The most commonly used analog divider circuit is the “inverted multiplier” configuration. As illustrated in Figure 46, an “inverted multiplier” analog divider can be configured with a multiplier operating in the feedback loop of an operational amplifier. The general form of the transfer function for this circuit configuration is given by:

$$V_O = -2.5V \times \left( \frac{R}{R+R_1} \right) \times \frac{V_{in}}{V_x}$$

Here, the multiplier operates as a voltage-controlled potentiometer that adjusts the loop gain of the op amp relative to a control signal, $V_x$. As the control signal to the multiplier decreases, the output of the multiplier decreases as well. This has the effect of reducing negative feedback which, in turn, decreases the amplifier’s loop gain. The result is higher closed-loop gain and reduced circuit bandwidth. As $V_x$ is increased, the output of the multiplier increases which generates more negative feedback — closed-loop gain drops and circuit bandwidth increases. An example of an “inverted multiplier” analog divider frequency response is shown in Figure 47.
Although this technique works well with almost any operational amplifier, there is one caveat: for best circuit stability, the unity-gain crossover frequency of the operational amplifier should be equal to or less than the MLT04's 8 MHz bandwidth.

Connection for Square Rooting

Another application of the “inverted multiplier” configuration is the square-root function. As shown in Figure 48, both inputs of the MLT04 are wired together and are used as the output of the circuit. Because the circuit configuration exhibits the following generalized transfer function:

$$\frac{V_O}{V_{IN}} = -2.5 \times \frac{R_2}{R_1} \times V_X$$

the input signal voltage is limited to the range $-2.5 \leq V_{IN} < 0$. To prevent circuit latchup due to positive feedback or input signal polarity reversal, a 1N4148-type junction diode is used in series with the output of the multiplier.

Voltage-Controlled Low-Pass Filter

The circuit in Figure 49 illustrates how to construct a voltage-controlled low-pass filter with an analog multiplier. The advantage with this approach over conventional active-filter configurations is that the overall characteristic cut-off frequency, $\omega_L$, will be directly proportional to a multiplying input voltage. This permits the construction of filters in which the capacitors are adjustable (directly or inversely) by a control voltage. Hence, the frequency scale of a filter can be manipulated by means of a single voltage without affecting any other parameters. The general form of the circuit’s transfer function is given by:

$$\frac{V_O}{V_{IN}} = -\left(\frac{R_2}{R_1} + \frac{1}{\frac{R_2 + R_1}{R_1} \cdot \frac{1}{5RC} + 1}\right)$$

In this circuit, the ratio of $R_2$ to $R_1$ sets the passband gain, and the break frequency of the filter, $\omega_L$, is given by:

$$\omega_L = \frac{R_1}{R_1 + R_2} \cdot \frac{V_X}{2.5RC}$$
then the output of the circuit has a pole at frequencies from 1 kHz to 100 kHz for $V_x$ ranging from 25 mV to 2.5 V. The performance of this low-pass filter is illustrated in Figure 20.

With this approach, it is possible to construct parametric biquad filters whose parameters (center frequency, passband gain, and Q) can be adjusted with dc control voltages.